Integral Equation Solution to the Skin Effect Problem in Conductor Strips of Finite Thickness

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Abstract—The skin effect of single and coupled conductor strips of finite thickness is analyzed using the dyadic Green’s function and the integral equation formulation. Galerkin’s method is used to solve the integral equation for the dispersion characteristics. The effects of the geometrical and electrical parameters on the conductor loss are investigated. Results are compared with the literature and shown to be in good agreement. This approach is very useful for analyzing the electrical properties of interconnects in high-performance computer circuitries.

I. INTRODUCTION

To calculate the conductor loss of microstrip lines, a perturbation method has usually been used. The surface currents for the lossless case are obtained first by either a quasi-TEM approximation [1]-[3] or a full-wave approach [4]. Then, the conductor loss is evaluated by using the surface resistance and the surface current. By using the surface resistance approximation, it is assumed that the strip thickness is much larger than the skin depth.

In [5], the equivalent surface impedance is used in the boundary condition from which an integral equation is derived. The conductor loss is then obtained by solving this integral equation. As in [4], it is assumed that the thickness of the strip is at least several skin depths, and is much smaller than the width of the strip. In [6], a complex resistive boundary condition is applied to solve for the propagation constant of thin superconducting striplines. It is assumed that the strip is thin compared with the superconducting penetration depth.

In [7] and [8], a skin loss expression is derived based on the incremental inductance rule, which was first proposed by Wheeler [9]. In this technique, the thickness of the conductors exposed to the electric field should be greater than several skin depths.

Finite element methods [3], [10]-[12] have been used to calculate the conductor loss. These approaches are based on either an electrostatic scalar potential [3] or a magnetic vector potential [10]-[12]. In the magnetic vector potential approach, only the longitudinal current component is considered. In [10], the ac resistance is derived from the power loss calculated from the current distribution in the cross section.

In [11], the thickness of the strip is assumed to be much smaller than the skin depth, and only surface current is considered.

In [13], a finite element method is used to calculate the attenuation constant of a copper microstrip at 77 K. The results are compared with the closed-form solution obtained by neglecting the effect of fringing fields [14]. In [15], a phenomenological equivalence method is proposed for characterizing a planar quasi-TEM transmission line with a thin normal conductor or superconductor strip. This method is based on various empirical formulas valid under different conditions.

In [16], a perturbation series and coupled integral equation approach is used to calculate the frequency-dependent resistance and inductance for quasi-TEM transmission lines with conductor strip of arbitrary cross section. A diffusion equation and a Laplace’s equation are solved interior and exterior to the conductor, respectively. Then, the boundary condition is imposed on the interface to obtain a coupled integral equation from which the frequency-dependent resistance can be obtained.

In [17], the ac resistance of cylindrical conductors is calculated by first assuming an axially independent TM mode excitation. Then the field expressions in the regions exterior and interior to the conductors are derived in terms of equivalent electric and magnetic surface currents. The continuity of tangential fields on the conductor surfaces are imposed to obtain the frequency-dependent resistance.

The skin effect becomes important in high-performance computer circuitries [18], [19] and superconductor transmission lines [13]-[15], [20]. In [14], the surface impedance for both the normal-state and the superconducting striplines are derived. It is assumed that the width of the stripline is much larger than the dielectric thickness so that the fringing field can be neglected. In [20], an approximate solution of propagation and attenuation constants for superconductor interconnects is presented. However, only the TM mode is considered, and the effects of interconnect cross section and the fringing field are not taken into account.

In this paper, an integral equation formulation using the dyadic Green’s function [21]-[23] is derived to solve for the attenuation relation of single and coupled conductor strips with finite thickness. In Section II, the integral equation formulation for a finite number of conductor strips is derived. In Section III, the Galerkin’s method is used to obtain the matrix eigenvalue equations. Numerical results and discussions are presented in Section IV.
II. INTEGRAL EQUATION FORMULATION

In Fig. 1, there are \( N \) conductor strips of arbitrary cross section embedded in layer (1) of a planar stratified medium. The whole structure is assumed to be uniform along the propagation direction \( y \). Then, the electric field in layer (1) can be represented by the dyadic Green's function and the equivalent conduction and polarization current in the conductor strips as

\[
E(r) = i\omega\mu_0 \int_V dV' \overline{G}_H(r, r') \cdot J_0(r')
\]

where \( J_0(r) = \Delta \sigma(r) E(r) \) with \( \Delta \sigma(r) = \sigma(r) - \sigma_\parallel \). The quantities \( \epsilon(r) \) and \( \sigma(r) \) are the permittivity and conductivity, respectively, in the cross section of the conductor strip; \( \epsilon_\parallel \) and \( \sigma_\parallel \) are the background permittivity and conductivity, respectively, in layer (1); and \( V \) is the space occupied by the conductor strips. The dyadic Green’s function \( \overline{G}_H(r, r') \) can be represented in the spectral domain as

\[
\overline{G}_H(r, r') = \frac{i}{8\pi^3} \int_{-\infty}^{\infty} dk_x dk_y dk_z e^{i \mathbf{k} \cdot \mathbf{r} - i \mathbf{k} \cdot \mathbf{r'}} \mathbf{g}_H(k_x, z, z') - \frac{2\pi}{k^2} \delta(r - r')
\]

where

\[
\begin{align*}
k_x &= \frac{\delta k_x}{k^2} + \frac{\delta k_y}{k^2} \\
r_y &= \frac{\delta k_x}{k^2} + \frac{\delta k_y}{k^2} \\
r_z &= \frac{\delta k_x}{k^2} + \frac{\delta k_y}{k^2}
\end{align*}
\]

Here, the time-harmonic convention of \( e^{i\omega t} \) is used. The first term on the right-hand side of (2) \( i \) is the principal value part of the dyadic Green’s function, and the second term \( \delta \) is the source dyadic. The source dyadic term shown in this spectral-domain solution is equivalent to using a thin disk as the exclusion volume in a principal-value integration over a current region in the space domain. \( \tilde{g}_H(k_x, z, z') \) is the Fourier transform of the principal value part of \( \overline{G}_H(r, r') \) with respect to \( r_y \).

For \( z > z' \), the explicit form of \( \tilde{g}_H(k_x, z, z') \) is given by [21]-[23]

\[
\tilde{g}_H(k_x, z, z') = \frac{1}{k_{1c}(1 - R_{1c}^{-1} R_{E}^{-1} e^{2ik_x h_1})} \left[ \hat{h}(k_{1c}) e^{-ik_x z} + R_{1c}^{-1} \hat{h}(-k_{1c}) e^{ik_x (2h_1 - z)} \right] + \frac{1}{k_{1c}(1 - R_{1c}^{-1} R_{E}^{-1} e^{2ik_x h_1})} \left[ \hat{\ell}(k_{1c}) e^{-ik_x z} + R_{1c}^{-1} \hat{\ell}(-k_{1c}) e^{ik_x (2h_1 - z)} \right]
\]

and for \( z < z' \), we have

\[
\tilde{g}_H(k_x, z', z') = \frac{1}{k_{1c}(1 - R_{1c}^{-1} R_{E}^{-1} e^{2ik_x h_1})} \left[ \hat{h}(k_{1c}) e^{-ik_x z'} + R_{1c}^{-1} \hat{h}(-k_{1c}) e^{ik_x (2h_1 - z')} \right] + \frac{1}{k_{1c}(1 - R_{1c}^{-1} R_{E}^{-1} e^{2ik_x h_1})} \left[ \hat{\ell}(k_{1c}) e^{-ik_x z'} + R_{1c}^{-1} \hat{\ell}(-k_{1c}) e^{ik_x (2h_1 - z')} \right]
\]

where \( z_1 \) and \( z_f \) are the local coordinates defined as \( z_1 = z + d_1 \), \( z_f = z' + d_1 \), and

\[
\hat{h}(\pm k_{1c}) = \frac{\delta k_x}{k_{1c}} \quad \hat{\ell}(\pm k_{1c}) = \frac{\delta k_x}{k_{1c}} + \frac{k_x}{k_{1c}}
\]

with \( \text{Im}(k_{1c}) > 0 \).
In (3), \( R_{\text{TM}} \) and \( R_{\text{TE}} \) are the reflection coefficients of the TM and the TE modes at the upper boundary of layer (1), and \( R'_{\text{TM}} \) and \( R'_{\text{TE}} \) are the reflection coefficients of the TM and the TE modes at the lower boundary of layer (1). They can be obtained recursively as

\[
R_{\text{TM}}(\alpha) = \frac{R_{\text{TM}}^{(1)}(\alpha) + R_{\text{TM}}^{(1)}(\alpha)e^{2ik_1z_h}}{1 + R_{\text{TM}}^{(1)}(\alpha)c^{2ik_1z_h}}, \quad \alpha = (\text{TE}, \text{TM})
\]

\[
R_{\text{TE}}(\alpha) = \frac{R_{\text{TE}}^{(1)}(\alpha) + R_{\text{TE}}^{(1)}(\alpha)e^{2ik_1z_h}}{1 + R_{\text{TE}}^{(1)}(\alpha)c^{2ik_1z_h}}, \quad \alpha = (\text{TE}, \text{TM})
\]

where \( R_{\text{TM}}^{(1)}(\alpha) \) and \( R_{\text{TE}}^{(1)}(\alpha) \) are the Fresnel reflection coefficients of the \( \alpha \) mode across the interfaces at \( z = -d_1 \) and \( z = -d_1 \), respectively. The explicit forms are

\[
R_{\text{TM}}(\alpha) = \frac{k_{z1} - k_{z1}e^{2ik_1z_h}}{k_{z2} + k_{z1}e^{2ik_1z_h}}, \quad R_{\text{TM}}(\alpha) = \frac{\epsilon_{z1}e^{ik_1z_h} - \epsilon_{z1}e^{ik_1z_h}}{\epsilon_{z2}e^{ik_1z_h} + \epsilon_{z1}e^{ik_1z_h}}.
\]

Substituting the dyadic Green's function in (2) into (1), we obtain

\[
E(r) + \frac{i\omega\mu_0\Delta\sigma(r)}{k_1^2} \cdot \bar{z}E_z(r) = -\frac{i\omega\mu_0}{4\pi} \int \int dV' \int \int_{-\infty}^{\infty} dk_z e^{ik_z(r-r')} \Delta\sigma(r') \cdot \tilde{\Phi}_{\beta}(r_z, \eta_z, \zeta_z) \cdot E_{\beta}(r')
\]

where the source dyadic contribution has been collected to be the second term on the left-hand side of (9). On the right-hand side of (9), the first (second) integral represents the contribution from the equivalent conduction and polarization current in the first (second) conductor strip.

In the next section, the Galerkin's method is used to solve the integral equations (8) and (9) for the dispersion relation \( \eta(\omega) \).

III. Numerical Solution

Consider a conductor strip with a rectangular cross section of width \( w \) and thickness \( t \). We first divide the width and thickness into \( N \) and \( M \) segments, respectively. The length of the \( n \)th segment in the \( x \) direction is \( w_n \), and the length of the \( m \)th segment in the \( z \) direction is \( t_m \), where \( w_1 + \cdots + w_N = w \) and \( t_1 + \cdots + t_M = t \). The center coordinate of the \( (n,m) \) cell, \( S_{nm} \), is denoted by \( (x_{nm}, z_{nm}) \) with \( 1 \leq n \leq N \) and \( 1 \leq m \leq M \).

The electric field of the \( p \)th eigenmode on the cross section \( S \) can thus be represented by a set of pulse basis functions as

\[
E_p(x, z) = \sum_{\beta = x, y, z} \sum_{n=1}^{N} \sum_{m=1}^{M} a_{p}^{(n,m)} \beta \bar{P}_\beta(x - x_n) R_m(z - z_m)
\]

where

\[
P_\alpha(x - x_n) = \begin{cases} 1, & x_n - w_n/2 \leq x \leq x_n + w_n/2 \\ 0, & \text{elsewhere} \end{cases}
\]

\[
R_m(z - z_m) = \begin{cases} 1, & z_m - t_m/2 \leq z \leq z_m + t_m/2 \\ 0, & \text{elsewhere} \end{cases}
\]
Substituting (10) and (11) into (8), we have

\[ \sum_{\beta=x,y,z} \sum_{n=1}^{N} \sum_{m=1}^{M} a_{nm} \beta P_{n}(x-x_{n})R_{m}(z-z_{m}) \]

\[ \cdot \left[ i \omega \mu_{0} \Delta \sigma_{nm} \delta_{\beta z} \right] \]

\[ = -i \omega \mu_{0} \sum_{\beta=x,y,z} \sum_{n=1}^{N} \sum_{m=1}^{M} a_{nm} \Delta \sigma_{nm} \]

\[ \cdot \int_{S_{mn}} d^{3}r \bar{P}_{n}(x'-x_{n})R_{m}(z'-z_{m}) \]

\[ \times \int_{-\infty}^{\infty} dk \, e^{ik(x'-x)} \delta_{\beta}^{(k,x',\eta,z,z')} \cdot \hat{\beta}, \quad \rho \text{ on } S \] (12)

where \( \delta_{\beta z} \) is the Kronecker delta function, which is equal to one when \( \alpha = \beta \), and is equal to zero when \( \alpha \neq \beta \), and \( \Delta \sigma_{nm} \) is the value of \( \Delta \sigma(\rho) \) calculated at \( (x_{n}, z_{m}) \).

For conductor strips of arbitrary cross section, we can approximate the cross section by a mosaic of rectangles, and a field expression similar to (10) can be obtained.

Next, we choose the same set of basis functions as the testing functions, and apply the Galerkin's method to (12). Taking the inner product of \( \hat{a} P_{n}(x-x_{n})R_{m}(z-z_{m}) \) with (12), we obtain

\[ -i \omega \mu_{0} \sum_{\beta=x,y,z} \sum_{n=1}^{N} \sum_{m=1}^{M} a_{nm} \Delta \sigma_{nm} \]

\[ \cdot \int_{-\infty}^{\infty} dk \, e^{ik(x'-x)} \delta_{\beta}^{(k,x',\eta,z,z')} \cdot \hat{\beta}, \quad \rho \text{ on } S \] (13)

where \( \alpha = x, y, z; 1 \leq r \leq N \) and \( 1 \leq q \leq M \). The eigenvalue \( \eta \) can thus be obtained by setting the determinant of the \( Z \) matrix in (18) to zero, i.e.,

\[ \det[Z(\omega, \eta)] = 0. \] (19)

Muller's method is then used to solve for the eigenvalue numerically.

To solve the integral equation (9) for two symmetrical conductor strips, we choose the same set of pulse basis functions as in (11) to represent the electric field on the cross section \( S_{1} \) as

\[ E_{\rho}(x) = \sum_{\beta=x,y,z} \sum_{n=1}^{N} \sum_{m=1}^{M} a_{nm} \beta P_{n}(x-x_{n})R_{m}(z-z_{m}), \]

\( \rho \text{ on } S_{1}. \) (20)

By symmetry, the electric field on the cross section \( S_{2} \) can be represented as

\[ E_{\rho}(x) = \sum_{\beta=x,y,z} \sum_{n=1}^{N} \sum_{m=1}^{M} P_{\alpha}^{m} a_{nm} \beta P_{n}(x+x_{n})R_{m}(z-z_{m}), \]

\( \rho \text{ on } S_{2}. \) (21)

where the subscript \( \xi \) in \( P_{\alpha}^{m} \) designates the even mode when \( \xi = e \), and the odd mode when \( \xi = o \). The definition of \( P_{\alpha}^{m} \) is

\[ P_{\alpha}^{m} = \left\{ \begin{array}{ll} 1, & (\xi, \beta) = (e,x),(o,y),(o,z) \\ -1, & (\xi, \beta) = (e,x),(o,y),(o,z) \end{array} \right. \] (22)
Substituting (20) and (21) into (9) for $\rho$ on $S_1$, we have

$$
\sum_{\beta=x,y,z} \sum_{n=1}^{N} \sum_{m=1}^{M} a_{nm}^\beta \hat{\beta} P_n(x-x_n) R_m(z-z_m)
\cdot \left[ i \omega \mu_0 \Delta \sigma_{nm} + \frac{k_i^2}{\delta \beta_2} \right]
= -\frac{\omega \mu_0}{4\pi} \sum_{\beta=x,y,z} \sum_{n=1}^{N} \sum_{m=1}^{M} a_{nm}^\beta \Delta \sigma_{nm}
\cdot \int_{S_m} dp \left[ P_n(x'-x_n) + l \hat{\beta} P_n(x'+x_n) \right] R_m(z'-z_m)
\cdot \int_0^\infty dk \epsilon_{k}(x-x') \cdot \hat{\beta}(k_x, \eta, z, z') \cdot \hat{\beta}, \quad \rho \text{ on } S_1.
$$

(23)

Owing to the symmetry of the structure, only the electric fields on $S_1$ need to be tested when applying the Galerkin's method. Taking the inner product of $\hat{P}_n(x-x_n) R_m(z-z_m)$ with (23) and utilizing the symmetry properties of the integrand with respect to $k_x$, we have

$$
-2\pi \omega \mu_0 \sum_{\beta=x,y,z} \sum_{n=1}^{N} \sum_{m=1}^{M} a_{nm}^\beta \Delta \sigma_{nm}
\cdot \int_0^\infty dk \epsilon_{k}(x-x') \cdot \hat{\beta}(k_x, \eta, z, z') \cdot \hat{\beta}, \quad \rho \text{ on } S_1.
$$

(24)

where $\alpha = x, y, z; 1 \leq r \leq N$ and $1 \leq q \leq M$; and

$$
W_{rq, \alpha \beta}^{(n)}(k_x, \eta) = \begin{cases} 
\cos k_x(x-x_n) + l \beta \cos k_x(x+x_n) \delta_{r\alpha} \delta_{q\beta} & (\alpha, \beta) = (x, x), (y, y), (z, z) \\
\sin k_x(x-x_n) + l \beta \sin k_x(x+x_n) \delta_{r\alpha} \delta_{q\beta} & (\alpha, \beta) = (x, y), (x, z), (y, x), (z, y), (z, z) 
\end{cases}
$$

(25)

Equation (24) is a matrix equation, and the eigenvalue $\eta$ can be obtained by setting the determinant of the matrix to zero.

IV. RESULTS AND DISCUSSIONS

In Fig. 2, we present the attenuation constant of a microstrip line of finite thickness embedded in a homogeneous medium. The results from a finite element method [13] are also presented for comparison. The deviation in the high-frequency range may be due to the truncation of structure in the finite element method.

Next, we present the propagation and attenuation constants of a stripline in Fig. 3. In this figure and the rest of the results, normal temperature is considered. Both copper (Cu) and molybdenum (Mo) are used to compare the effect of conductivity since these two materials are commonly used in
the fabrication of interconnects in computer circuitries. For this structure, we divide the strip cross section into 14 by 6 small rectangles. The size of the rectangles closer to the strip surface is chosen to be smaller than the size of those farther away from the surface. Note that at the frequency of 100 MHz, the skin depths of Cu and Mo are about 6.54 μm and 11.49 μm, respectively. It is also found that although the magnitude of the transversal current is much smaller than that of the longitudinal (y) component, the results of the attenuation constant become unreasonable when the transversal currents are neglected. The computation was done by using an IBM 3090/600E mainframe computer, and the computation time is about a few seconds to obtain each curve.

In Fig. 3, it is observed that the propagation constant deviates slightly from that of the TEM mode. The attenuation constant approaches a constant as frequency is reduced, and becomes proportional to the square root of frequency at higher frequencies. The result for Mo strip and Mo ground plane is close to that for Mo strip and Cu ground plane. This implies that the conductor loss is mainly contributed by the strip.

In Fig. 4, we present the attenuation constant of a stripline where the strip is located closer to the lower ground plane. The attenuation constant is larger than that of the corresponding case in Fig. 3. Because the strip is closer to the lower ground plane, the field strength increases below the strip. Although the field strength is smaller between the strip and the upper ground plane than in Fig. 3, the overall conductor loss is increased. The propagation constant is close to the results in Fig. 3(a), and is not presented.

In Fig. 5, the cross section of the structure is scaled down by a factor of 10, and the frequency range is scaled up proportionally. It is observed that the propagation constant deviates more from that of the TEM mode than in Fig. 3. Meanwhile, the attenuation constant is much larger than that in Fig. 3.

In Fig. 6, we present the attenuation constant for a stripline with a square cross section of the same area as the cross section of the stripline in Fig. 3. The attenuation constants in both cases are roughly the same.
In Fig. 7, the attenuation constants of two coupled striplines are presented. The separation $s$ between the two strips is defined as the shortest distance between them. The attenuation constant of the odd mode is larger than that of the even mode owing to the difference of field distributions.

In Fig. 8, we present the propagation and attenuation constants of both modes as a function of the separation between the two strips. It is observed that the results for the even mode are less sensitive to the separation than the odd mode. This is because the field distribution of the odd mode changes more drastically than that of the even mode as the separation is changed.

The attenuation constants of two coupled striplines in an up-down arrangement are presented in Fig. 9. Again, the attenuation constant of the odd mode is larger than that of the even mode. The propagation constants for both modes are very close to that in Fig. 3(a) and hence are not presented.

Next, we present the attenuation constant for a symmetrical structure consisting of four strips as shown in the inset of Fig. 10. There are four fundamental modes, indicated by $ee$, $eo$, $oe$, and $oo$. The results for $ee$ and $oo$ modes are very close to those for $ee$ and $oo$ modes in Fig. 8, respectively, and hence are not presented.
Table 1 lists the even/odd parity of field components. The first symbol indicates the symmetry with respect to the horizontal center line, and the second symbol indicates the symmetry with respect to the vertical center line. The even/odd parity of all the field components is shown in Fig. 11, where the + (–) sign represents an even (odd) symmetry with respect to the center line.

As shown in Fig. 10, the attenuation constant of the ee mode is the smallest, and that of the oo mode is the largest. This again is due to the field distributions of different modes. The propagation constants of these four modes are all close to that of the TEM mode for a single stripline.

In Fig. 12, we present the results of four different modes as a function of horizontal separation. It is observed that the ee and oe modes are less sensitive to the horizontal separation because these two modes have an even symmetry with respect to the vertical center line.

V. Conclusions

An integral equation formulation utilizing the dyadic Green’s function is proposed to calculate the conductor loss in a rigorous way. Galerkin’s method is used to solve the integral equation for the dispersion relation where the conductor loss is incorporated in the attenuation constant. The attenuation properties for different stripline structures used in the packages of high-performance computer circuitries are presented.

References


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